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Description

Circuit arrangement and method for protecting an integrated semiconductor circuit

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The invention relates to a circuit arrangement for protecting an integrated semiconductor circuit comprising a protection circuit, which contains a thyristor structure and is connected between an element
10 to be protected and a reference potential, and comprising a control circuit for driving the protection circuit, and also to a corresponding method for protecting an integrated semiconductor circuit.

15 Integrated semiconductor circuits (ICs) can be damaged by transient pulses or overvoltages, which are coupled in via terminals (pads) or directly in lines, such that they become nonfunctional or are even destroyed. Such pulses or overvoltages may occur for example in the
20 event of so-called electrostatic discharges (ESD). High voltages and high currents, associated with transient or ESD disturbances, cause high disturbing powers to occur.

25 Such a pulse (e.g. burst) may also occur in many fields of application, e.g. automotive engineering. In automotive engineering, by way of example, there is the requirement that circuits of this type which have to function in the high-voltage range up to 90 volts or
30 above are also to be designed for significantly higher disturbance pulse levels.

For high-voltage applications produced by means of high-voltage processes, provision is usually made of
35 protection devices that are initiated or triggered by an electrical breakdown. The breakdown voltages must be significantly greater than the maximum permissible operating voltages of the application circuit to be protected. Only then is it possible to guarantee an

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undisturbed functionality of the integrated circuit. In the case of a fault, e.g. when an impermissibly high voltage is present, this overvoltage is dissipated to reference potential or ground by the protection circuit and downstream assemblies are thus protected from the high voltage.

One alternative for such breakdown-based protection concepts is an active circuit for protecting an integrated circuit, comprising a combination of an active trigger circuit with a known protection device such as a thyristor or a bipolar or MOS protection transistor.

Active circuits for protecting the IC are often triggered by the rise of the transient signal. In this case, the signal rise per unit time is detected and a protection transistor or a protection circuit is turned on by means of a drive circuit.

In the case of a fault, the protection circuit may accordingly be understood as an actively triggered overvoltage or overcurrent surge arrestor. A fast activation of the protection circuit is necessary in the case of a fault.

Short switch-on times and a precise switch-on threshold of the protection circuit for the integrated circuit and the protective effect thereof for different forms of disturbance pulses are important aspects of the product specification and constitute a competitive advantage.

US 5,982,601 discloses a thyristor (SCR - silicon control rectifier) for ESD protection, which is triggered directly by the transient signal. The thyristor is realized in the semiconductor arrangement in a manner known per se by means of an n-type well, a

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p-type well and highly doped n-type and p-type regions. The transient voltage is detected by means of an RC element. By means of inverters connected downstream, the voltage level detected at the capacitance is
5 converted into a control signal which drives the base of the pnp transistor of the thyristor structure. As soon as the output current of the then active pnp transistor generates a sufficiently large voltage drop at a resistor, the npn transistor of the thyristor
10 structure turns on, so that the transient pulse is dissipated from the pad potential of the I/O pin to reference potential through the low-impedance thyristor path. The thyristor then automatically remains turned on until its current falls below the holding current
15 and the turn-off condition is met.

The invention is based on the object of specifying a circuit arrangement and a method for protecting integrated semiconductor circuits which enable an
20 improved behavior. Furthermore, the intention is to specify a circuit arrangement and a method which are in particular also suitable for high-voltage processes or for high-voltage applications.

25 The invention achieves this object by means of the features of patent claims 1 and 19, respectively.

The invention has the advantage that the circuit arrangement as an actively triggered protection circuit
30 and the corresponding method enable the thyristor structure to be turned on rapidly. Furthermore, the invention can be integrated in high-voltage applications which are produced using high-voltage processes.

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The dependent patent claims relate to advantageous configurations and developments of the invention.

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The invention is explained in more detail below on the basis of exemplary embodiments in connection with the figures. Identical or identically acting elements are provided with the same reference symbols in the
5 figures.

In the figures:

figure 1 shows a schematically illustrated circuit
10 arrangement comprising protection circuit and control or trigger circuit,

figure 2 shows a second schematically illustrated
15 circuit arrangement comprising protection circuit and trigger circuit,

figure 3 shows a third schematically illustrated
20 circuit arrangement comprising protection circuit and trigger circuit,

figure 4 shows a fourth schematically illustrated
circuit arrangement comprising protection
circuit and trigger circuit,

25 figure 5 shows a further schematically illustrated
circuit arrangement comprising protection
circuit and trigger circuit, and

figure 6 shows a schematic cross section through a
30 structure for realizing the thyristor in a
high-voltage process.

In figure 1, the invention is elucidated in greater
detail in principle and on the basis of two exemplary
35 embodiments. In accordance with figure 1a, a terminal
PV is connected to a line LV, which is at a potential
VV. The potential VV may be e.g. the positive supply
potential VDD or the potential of an input/output

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terminal (I/O pad). The terminal PV and the line LV are to be protected against transient pulses or against overvoltage. Said overvoltage must be dissipated to a reference potential VB, which may be the ground potential, by way of example. The line LB carrying the reference potential VB is connected to the terminal PB.

The actual task of dissipating disturbance pulses or overvoltages is fulfilled by the protection circuit PC, which is designated as SCR in all the exemplary embodiments. The protection circuit PC or SCR is controlled or triggered by a control circuit TC, which is connected to the terminals PV and PB on the input side. The control circuit TC contains a detector circuit, which is able to identify the transient pulses occurring at the terminal PV or on the line and to generate control signals for the protection circuit PC or SCR.

The control circuit TC generates a plurality of control signals which in each case drive an active element of the protection circuit PC or SCR. In figure 1 these are the signals CTL and CTH, which drive the transistors T1 and T2, respectively. The active elements of the protection circuit PC or SCR are generally connected up in such a way that, in the event of driving by the control signals of the trigger or control circuit TC, they produce a low-impedance connection between the line LV or the terminal PV and the reference potential VB. In this case, the protection circuit PC or SCR may also dissipate higher currents to reference potential VB.

In the typical application situation in figure 1, the protection circuit PC or SCR contains a thyristor structure. A thyristor is a four-layer component, represented as two bipolar transistors connected up to one another in the equivalent circuit diagram. In the

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case of a fault, the control circuit TC actively drives the two transistors T1 and T2 (T10 and T20 in figure 4 and figure 5) of the thyristor structure of the protection circuit with two control signals. For this purpose, currents are injected directly into the two base-emitter junctions.

The turn-on of the protection circuit PC or SCR by means of control signals for the active elements of the protection circuit which, in their interconnection, have to produce the low-impedance connection between the line LV and the line LB is thus initiated in a targeted manner. As a result, it is possible to take the protection circuit PC or SCR into the turned-on state precisely and rapidly. This leads to an improved response behavior of the protection circuit and thus to better protection of the integrated semiconductor circuit, which is illustrated symbolically in figure 1 on the basis of the terminals PB and PV and the lines connected thereto.

A first concrete exemplary embodiment of the invention is illustrated in accordance with figure 1b). The protection circuit is embodied as a thyristor SCR having the two transistors T1 and T2. T1 is a pnp transistor connected by its emitter to the voltage-carrying line LV, while T2 is an npn transistor connected to the reference potential VB on the emitter side. The collectors of the two transistors are cross-connected to the base of the respective other transistor. In an integrated circuit, a transistor structure of this type may be realized in a manner known per se by an n-type and p-type well, respectively, having well resistors RN and RP, respectively, and highly doped regions correspondingly arranged therein, see figure 6 and schematically figures 3 to 5. The resistors RN and RP are not depicted in figures 1 and 2 for the sake of a better

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understanding of the mode of operation of the invention.

In figure 1b), the control circuit is realized by a
5 detector circuit with inverters connected downstream.
The detector circuit is embodied as an RC element
comprising the series circuit formed by a capacitance
C1 and a resistor R1, said series circuit being
connected to the lines LV and LB and the corresponding
10 terminals PV and PB. Inverters are connected downstream
of the connecting node between the capacitance C1 and
the resistor R1, which inverters, on the output side,
in each case drive the bases of the transistors T1 and
T2. In this case, the inverter I1 is connected to the
15 base of the transistor T1 and two series-connected
inverters I2 and I3 are connected to the base of the
transistor T2. The inverters are necessary in order to
convert the potential present at the connecting point
between the capacitance C1 and the resistor R1 into
20 defined control signals CTL and CTH, which drive the
transistor elements of the thyristor SCR.

The detector circuit comprising capacitance C1 and
resistor R1 forms, as an RC element, a complex voltage
25 divider, at the center tap of which the voltage rise of
the disturbance pulse is detected. In the fault
situation of a transient pulse, the capacitance C1
attains low impedance, so that a high potential is
established at the output point of the detector
30 circuit. As soon as the voltage reaches the switching
threshold of the inverter I1, the output signal CTL
thereof switches to low potential, so that the pn
junction between emitter and base of T1 exceeds the
switching threshold and T1 turns on.

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On the other hand, the series-connected inverters I2
and I3, which convert the voltage signal detected at
the tapping node of the detector circuit into a defined

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control signal CTH for driving the npn transistor T2, are connected in parallel with I1. Consequently, T2 switches over into the conducting state virtually simultaneously with T1. As a result, the thyristor SCR becomes conducting and the transient pulse present on the line LV or the terminal PV can be dissipated to reference potential.

The exemplary embodiment in accordance with figure 1c) differs from the exemplary embodiment according to figure 1b) by virtue of the fact that the detector circuit comprising the capacitive and resistive components is connected to the terminals PV and PB in a reversed direction. In this case, the resistor R11 is connected to the terminal PV and the capacitance C11 is connected to the terminal PB. Consequently, the voltage conditions at the output of the detector circuit, namely the connecting point between R11 and C11, are reversed, so that the transistors T1 and T2 must also be driven differently. Therefore, the series circuit comprising the inverters I4 and I5 is connected downstream of the output of the detector circuit in order to drive the transistor T1. In parallel with said inverters, the inverter I6 is connected downstream of the output of the detector circuit, and drives the transistor T2.

In the fault situation of a transient pulse, the capacitance C11 attains low impedance, so that a low potential is established at the output point of the detector circuit. The inverter I6 converts said low potential into a voltage required for activating the transistor T2, or a corresponding control current. On the other hand, the series-connected inverters I4 and I5 convert the output voltage at the capacitance C11 into a control signal having low potential or a corresponding current, so that the transistor T1 turns on.

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The detector circuit is embodied as an RC element in the exemplary embodiments of figure 1, but the invention is not restricted thereto. Other embodiments of the detector circuit may also be expedient, as long as the essential function, namely the identification of a transient pulse to be dissipated on the voltage-carrying line LV and the generation of control signals for activating the active elements or semiconductor junctions of the protection circuit, the transistors of the thyristor SCR in the exemplary embodiment, are functionally fulfilled.

What is crucial is that the transient signal is identified, on the one hand, and the thyristor SCR is not triggered during normal operation, on the other hand. The time constant of the RC element determines on the one hand the identification of a transient pulse and also, on the other hand, the time during which the detector circuit is active. A pulse is identified and detected as long as the rise time of the transient disturbance is less than the time constant of the RC element. On the other hand, the time constant, after the pulse has decayed, determines the time after which the detector circuit becomes inactive and switches off or reverts to normal operation again.

For this purpose, in the exemplary embodiments of figure 1, the RC element is set with its time constant such that these conditions are met. Since, in these exemplary embodiments, the thyristor is only triggered in the case of a fault, but need not be switched off, it suffices to identify the rising edge of a transient pulse.

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In the case where the RC element respectively has a small capacitance, for example realized as gate oxide capacitance, the impedance of said capacitance becomes

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low during transient processes, so that, in the exemplary embodiment of figure 1b), the output of the RC element is brought to high potential very rapidly, while the output of the detector circuit in figure 1c) is brought to low potential very rapidly. In the case of small voltage changes and in the case of DC voltage, the impedances of the capacitances of the RC element act as high-impedance components in both exemplary embodiments, so that in figure 1b) the output of the detector circuit is held at low potential, while it is held at high potential in the circuit according to figure 1c).

The circuit arrangements of figure 2 show a second exemplary embodiment of the invention. In contrast to the exemplary embodiments shown in figure 1, an additional circuit is provided in the circuit arrangements from figure 2, which additional circuit determines how long the control circuit remains active. It is thereby possible to ensure that the control signals of the control circuit activate the thyristor SCR at least until the transient pulse on the line LV or the terminal PV has certainly decayed.

In comparing the exemplary embodiment according to figure 2a) with the exemplary embodiment of figure 1b) the difference is that an additional circuit is arranged between the first RC element comprising the elements C12 and R12, which detects the transient pulse on the voltage-carrying line LV or the terminal PV and activates the control circuit, and the inverters for driving the thyristor SCR. In this case, firstly the inverters I1, I2 and I3 according to the exemplary embodiment of figure 1b) correspond in this order to the inverters I20, I30 and I40 in figure 2a). The function of these inverters in figure 2a) is identical to that of the inverters of the first exemplary embodiment, but the dimensioning and the realization of

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the inverters may be embodied in a different manner.

As an element of the additional circuit, an inverter I10 is connected downstream of the output of the first RC element comprising R12 and C12, and drives a PMOS transistor P10. On the output side, said transistor is connected to the voltage-carrying line LV, on the one hand, and to the inputs of the inverters I20 and I30, on the other hand. There is furthermore connected to the latter connecting point the parallel circuit of a second RC element comprising the capacitance C21 and the resistor R21, which are connected by their other terminal in each case to the reference potential VB or the line LB.

15

In the case of a transient disturbance on the line LV or the terminal PV, this is identified by the first RC element. The output of said first RC element, which drives the inverter I10, assumes high potential in the case of a fast pulse rise through the capacitance C12 then at low impedance, so that the inverter I10 is brought to low potential on the output side. As in the exemplary embodiments of figure 1, the rise time of the transient disturbance on the line LV must in this case be shorter than the time constant of the first RC element.

The output of the inverter I10, which is then at low impedance, activates the PMOS transistor P10, the output of which puts the inverter inputs of the inverters I20 and I30 at high potential. As already explained on the basis of the exemplary embodiment of figure 1b) the transistors T1 and T2 are subsequently activated, so that the thyristor SCR becomes conducting and can dissipate the pulse on the line LV to reference potential.

The time constant of the second RC element comprising

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the elements C21 and R21 can be set independently of the time constant of the first RC element and in this situation determines how long the control circuit remains active and generates control signals to the transistors T1 and T2. As long as P10 remains turned on, the inverters I20, I30 and I40 are able to generate the control currents for turning on the transistors T1 and T2. As soon as P10 switches off, e.g. because the transient pulse flattens out and the time constant of the first RC element becomes shorter than the voltage changes on the line LV, the connecting node between the inputs of the inverters I20 and I30 and the second RC element is discharged to reference potential via said RC element and the time constant thereof. The time constant of the second RC element is typically set such that the control circuit outputs the control signals to the thyristor for as long as the transient disturbance lasts. This means that the time constant of the second RC element is greater than the time constant of the first RC element. In this way, different transient pulse forms can be detected and dissipated by means of the first and second RC elements. Furthermore, the time constants of the two RC elements can be optimized with regard to their function independently of one another.

Figure 2b) differs from the exemplary embodiment of figure 2a by virtue of the fact that the inverters are embodied in concrete terms as CMOS inverters I11, I21, I31 and I41.

It goes without saying that the exemplary embodiment with a second RC element can also be adapted to the first exemplary embodiment according to figure 1c.

The actively triggered protection circuit concepts described above make use of inverters. The inverters supply the voltages or currents with the necessary short signal rise times in order to trigger the actual

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protection circuit.

The use of inverters in high-voltage applications is in turn not completely unproblematic. High-voltage components produced using high-voltage processes often have asymmetrical operating parameters or operating conditions as a result of the nature of the high-voltage process, in particular the multiple isolation wells. By way of example, the maximum permissible drain-source voltage of a MOS transistor may be considerably higher than the corresponding maximum permissible gate-bulk voltage. Therefore, specific component configurations, such as e.g. standard inverters, cannot be produced for the possible voltage ranges.

In accordance with a third exemplary embodiment of the invention, the control circuit in figure 3 is realized by a detector circuit with control transistors TH1 and TL1 connected downstream as output switching elements. The detector circuit contains two subcircuits, one of which drives the transistor T1 and the other of which drives the transistor T2. In principle, in this case, too, each detector subcircuit contains, for transient identification, an RC element comprising the series circuit formed by a capacitance and a resistor, said RC element being connected to the lines LV and LB and the corresponding terminals PV and PB.

Each detector subcircuit comprising a capacitance and resistor forms, as an RC element, a complex voltage divider, at the center tap of which the voltage rise of the disturbance pulse is detected. In the fault situation of a transient pulse, as described, the (complex) impedance of the capacitance becomes low ("low impedance"), so that a low or high potential is established at the output node of the detector circuit depending on the polarity of the RC circuit. As soon as

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the node voltage reaches the switching threshold of the detector transistor (TD1 and TD2, respectively), the latter turns on and generates at its output a potential which can drive and turn on the control transistors (TH1 and TL1). The output voltages of the switched control transistors have the effect that the pn junction between emitter and base of T1 and T2, respectively, exceeds the switching threshold and the protection circuit turns on.

10

The detector subcircuit for driving T1 is embodied from the series circuit formed by a capacitance C13 and a resistor R13. The transistor TD1 is connected downstream of the connecting node between the capacitance C13 and the resistor R13. TD1 is embodied as a p-channel transistor. TD1 drives the n-channel control transistor TL1 on the output side. TL1 is connected to the base of T1 on the output side.

20 In the case of a transient disturbance, the impedance of C13 becomes low, so that TD1 turns on and the output of TD1 assumes high potential, in particular VV, and activates TL1. The output of TL1 and the base of T1 are thereby connected to reference potential VB and T1 turns on.

The detector subcircuit for driving T2 differs from the detector subcircuit for driving T1 by virtue of the fact that the RC series circuit comprising the capacitive component and the resistive component is connected to the terminals PV and PB in a reversed direction. In this case, the resistor R2 is connected to the terminal PB and the capacitance C2 is connected to the terminal PV. Consequently, the voltage conditions at the output of the detector circuit, namely the connecting point between R2 and C2, are reversed, so that the transistor T2 must also be driven differently.

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The transistor TD2 is connected downstream of the connecting node between the capacitance C2 and the resistor R2. TD is embodied as an n-channel transistor.

5 TD2 drives the p-channel control transistor TH1 on the output side. TH1 is connected to the base of T2 on the output side.

In the case of a transient disturbance, the impedance

10 of C2 becomes low, so that TD2 switches and the output of TD2 assumes low potential, in particular VB, and can activate TH1. The output of TH1 and the base of T2 are thereby connected to high potential VV and T2 turns on.

15 Other embodiments of the detector circuit may also be expedient as long as the essential function described above is fulfilled.

What is crucial is that the transient signal is

20 identified, on the one hand, and the thyristor SCR is not triggered during normal operation, on the other hand. The time constant of the RC element determines the identification of a transient pulse.

25 T2 then switches over into the conducting state simultaneously or virtually simultaneously with T1. As a result, the thyristor SCR becomes conducting and the transient pulse present on the line LV or the terminal PV can be dissipated to reference potential. It goes

30 without saying that it is also possible to set different time constants if this necessity should arise.

The elements R3, C3 and R4, C4 illustrated in figure 3

35 determine how long the control circuit remains active or after what time the protection circuit SCR is switched off again. It is thereby possible to ensure that the control signals of the control circuit

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activate the thyristor SCR at least until the transient pulse on the line LV or the terminal PV has certainly decayed.

- 5 The parallel circuit of a further RC element comprising the capacitance C3 and the resistor R3 is thus connected between the base terminal of the transistor TL1 and reference potential VB. The parallel circuit of an RC element comprising the capacitance C4 and the
10 resistor R4 is connected between the base terminal of the transistor TH1 and high potential VV.

The time constants of the RC element comprising the elements C3, R3 and C4, R4, respectively, can be set
15 independently of the assigned time constant of the RC element comprising C13, R13 and C2, R2, respectively, and determine how long the control circuit remains active and the control signals are present at the transistors T1 and T2. As long as TL1 and TH1 remain
20 turned on, TL1 and TH1 can generate the control currents for turning on the transistors T1 and T2, respectively.

As soon as the transient pulse flattens out and the
25 time constant of the RC elements comprising C13, R13 and C2, R2, respectively, become shorter than the voltage changes on the line LV, the inputs of TD1 and TD2 are connected to high potential and reference potential, respectively, via said RC elements and their
30 time constants. TD1 and TD2 switch off.

The time constants R3, C3 and R4, C4 are typically set such that the control circuit outputs the control signals to the protection circuit for as long as the
35 transient disturbance lasts. According to the time constants of C3 and R3, and C4 and R4, respectively, with transistors TD1 and TD2, respectively, switched off, the inputs of the control transistors TL1 and TH1,

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respectively, are inhibited and the control currents of T1 and T2 are switched off.

Different transient pulse forms can be detected and
5 dissipated by way of the setting of the time constants. Furthermore, the time constants of the RC elements can be optimized with regard to their function independently of one another.

10 Figure 4 shows a fourth exemplary embodiment of the invention, which differs from the exemplary embodiment of figure 3 essentially by virtue of the fact that additional gate driver transistors are used. An improvement of the switching behavior of the control or
15 trigger transistors TH10 and TL10 thus becomes possible.

As a result of the use of the gate driver transistors, it is necessary, in comparison with figure 1, to adapt
20 the elements of the control circuit to the polarity of the control signals. The use of transistor T11 as a gate driver for TD10 requires a polarity reversal of the detecting RC element, so that C10 is connected to VV and R10 is connected to VB. The n-channel driver
25 transistor T12 in the output circuit of TD10 drives the p-channel switching transistor TH10 and the latter in turn drives T20. The same applies correspondingly to the second detector subcircuit for R20, C20 and the driver transistor T21, which form the detector input
30 circuit for the detector transistor TD20. The p-channel driver transistor T13 in the output circuit of TD20 drives the n-channel switching transistor TL10 and the latter in turn drives T10. For the design of the RC elements, the explanations with respect to figure 1 are
35 correspondingly applicable.

For the exemplary embodiments of figures 3 and 4, the control circuit for detecting the transient event and

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for driving T1 and T2 is constructed from two partial circuits or subcircuits which are assigned separately to each of the transistors T1 and T2. The separate embodiment of the subcircuits of the control circuit
5 enables these partial circuits to be dimensioned and optimized independently.

The further exemplary embodiment in accordance with figure 5 differs from the exemplary embodiment of
10 figure 4 by virtue of the fact that the two control transistors TL10 and TH10 with driver transistors T13 and T12, respectively, connected upstream use the same detector circuit. In this case, T12 serves not only for driving TH10, but also for driving the gate driver
15 transistor T13 and the switching element TL10 connected downstream. The elements C10, R10, T11, TD10 and also C30, R30 are provided only once in the protection circuit. The elements R20, C20, R40, C40, TD20 and T21 of the second detector subcircuit can thus be omitted.

20 In the exemplary embodiment in accordance with figure 5, although independent dimensioning of the detector partial circuits is omitted, because the detector circuit is present only once, independent
25 dimensioning of the detector subcircuits is in many cases not desirable or not necessary if identical time constants are desired for the driving of T10 and T20. On the other hand, the circuit enables the significant reduction and the optimization of the area requirement
30 of the protection circuit on the semiconductor chip. It is still possible, however, to independently dimension and optimize the control transistors TH10 and TL10 and their driver transistors T12 and T13, respectively.

35 In accordance with this embodiment of the invention, as a result of the use of individual transistors in the control circuit no inverters are required in order to trigger the protection circuit SCR. It is possible to

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optimize the individual transistors which are used as switching elements of the control circuit in any process for producing the integrated circuit, in particular in high-voltage processes, but also in
5 standard processes. Consequently, an optimized protection circuit can be produced even using a high-voltage process as well as in low-voltage processes.

It goes without saying that the invention is not
10 restricted to the use of MOS transistors as switching elements. Bipolar transistors may likewise be used as switching elements.

Further embodiments of the control circuit and of the
15 protection circuit are possible and, although not illustrated, are included within the scope of protection of the invention.

The structure of the protection arrangement in the
20 semiconductor component is specified by the exemplary embodiment in accordance with figure 6. A lightly p-doped well 10 is arranged in the semiconductor, which is not illustrated in specific detail. The well 10 may also be the substrate of the semiconductor. An n-doped
25 well 20 is arranged in the well 10. The thyristor made from T1 and T2 is embedded in the n-type well 20 using a high-voltage process in the exemplary embodiment. In this case, the n-type well 20 serves for controlling the high voltages that occur.

30 Highly doped regions having p-type or n-type conductivity are arranged in the well 20; they can be produced in a customary manner for example by implantation or diffusion. The highly doped n-type
35 region 21 and also the highly doped p-type region 22 may be connected separately to a potential, but they must have the same potential during operation. For this purpose, they are in each case connected to the high

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potential VV. The highly doped n-type region 23 is connected to the output CTL of the control circuit.

A p-doped well 30 is likewise arranged in the n-type well 20. Two highly doped p-type regions 31 and 33 and also a highly doped n-type region 32 are arranged in said well 30. These regions may be produced in a conventional manner by implantation or diffusion in a similar manner to the highly doped regions of the n-type well. The regions 32 and 33 may be connected separately to a potential, but they must have the same potential during operation. For this purpose, in the example they are in each case connected to the reference potential VB. The region 31 is connected to the output CTH of the control circuit.

Field plates P11 and P12 made of polysilicon (typically as a poly1 layer) are formed above the boundary regions of the n-type well 20 and the p-type well 30. The field plates serve for controlling the electric field at the high operating voltages and increase the breakdown voltage of the arrangement. This results in lower susceptibility of the circuit to incorrect triggering.

The parasitic thyristor structure comprising the transistors T1 and T2 is depicted in the n-type well and p-type well, respectively. Accordingly, the collector of the npn transistor T2 is produced between the region 21 with downstream resistance RN of the n-type well 20 and the region 23. The base is produced from the region 31 and the collector T1 and is connected to reference potential VB via the resistance RP of the p-type well 30. The base of said transistor T2 is connected to the region 31 as a control terminal to which the control signal CTH for switching the transistor on and off can be applied. The emitter is produced as region 32.

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The base of the pnp transistor T1 is produced between the region 21 and the downstream bulk resistance RN of the n-type well 20 and the collector of the transistor T2 or the region 23 at which the signal CTL is present.

5 The collector of T1 is produced between the terminal 33 with downstream bulk resistance RP of the p-type well 30 and the region 31. The emitter of the transistor T1 is connected to the region 22. The control signal CTL serves for switching the transistor T1 on and off.

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The control lines or control signals CTL and CTH are firstly put at low potential (region 23) and high potential (region 31), respectively, in order to switch the transistors T1 and T2 on. A base current is
15 respectively provided in this case for the pnp transistor and the npn transistor. The base currents switch the respective transistor on and thus trigger the thyristor. The protection function is thus in operation between the lines LV and LB.

20

In order to switch the thyristor off, the region 23 is connected to high potential via the terminal CTL after the control transistor TL1 has been switched off, by means of the bulk resistance RN, and the region 31 is
25 connected to low potential via the terminal CTH after the control transistor TH1 has been switched off, by means of the bulk resistance RP. The transistors T1 and T2 thus turn off and thus turn off the thyristor.